

# Circular antenna array beamforming for ultra wideband short pulse applications

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# Contents

Circular  
antenna  
array  
beamforming  
for UWB

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Shalaby

## Contents

Introduction  
and  
Motivation

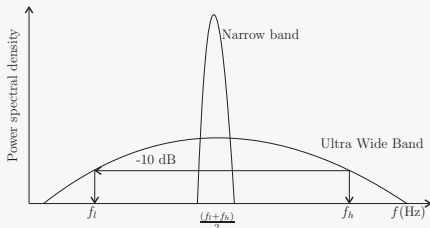
Narrowband  
Beamforming

UWB  
Beamforming

Simulation  
Process

Future Work

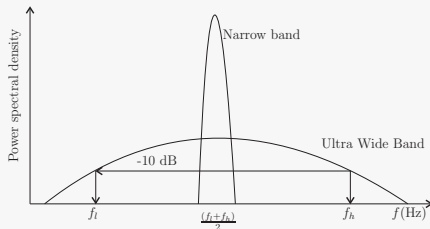
- 1 Introduction and Motivation
- 2 Narrowband Beamforming
- 3 UWB Beamforming
- 4 Simulation Process
- 5 Future Work



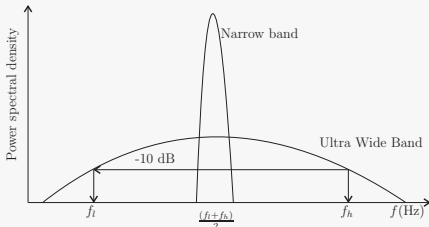
- Enormous bandwidth and therefore according to the Shannon's formula

$$C = B \log_2 (1 + SNR)$$

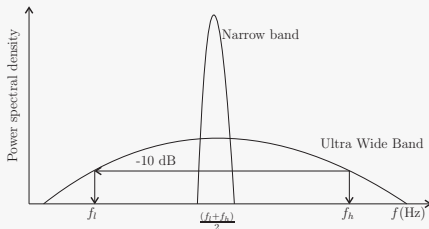
offers very high data rates.



- No need for expensive licensing fees as it can co-exist with existing radio services due to its low power level



- Immune against detection and interception (as it appears like background noise), has all-weather capabilities and higher angular resolution (very attractive to the military)



- Baseband technique as the pulse can propagate well without any need for additional modulation stages.



# Typical Problems and solution

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antenna  
array  
beamforming  
for UWB

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Contents

Introduction  
and  
Motivation

Narrowband  
Beamforming

UWB  
Beamforming

Simulation  
Process

Future Work

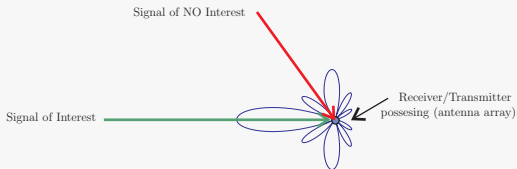
## Problems

Like any other wireless technology UWB suffers from multipath propagation and different kind of interferences leading to decreased data rate level.

## Solution

Array Beamforming

# Why Array Beamforming?



Based on exploiting the physical phenomena of the interference of Electromagnetic waves.

- Constructive interference towards Signal of Interest.
- Destructive interference towards Signal of NO Interest.
- implemented using antenna arrays.
- The extent depends on the phase shift  $kl$ .
- The direction of the mainbeam and the nulls can be changed electronically





# Why Circular Arrays?

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array  
beamforming  
for UWB

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Contents

Introduction  
and  
Motivation

Narrowband  
Beamforming

UWB  
Beamforming

Simulation  
Process

Future Work

Unique Features: Circular Symmetry and lack of edge elements

Consequences: It can scan a beam azimuthally through  $360^\circ$  with little change in beamwidth and sidelobe levels in contrast to linear arrays as we see in the next diagram

# Comparison bet. Linear and Circular Array Radiation Patterns



Circular antenna array beamforming for UWB

Mohammed Shalaby

Contents

Introduction and Motivation

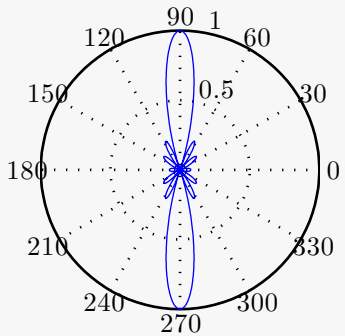
Narrowband Beamforming

UWB Beamforming

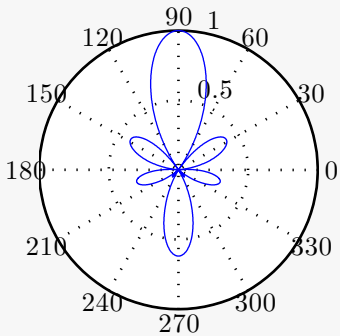
Simulation Process

Future Work

### Linear Array



### Circular Array



$\phi_o=90 ; N= 8$  in both arrays

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Circular antenna array beamforming for UWB

Mohammed Shalaby

Contents

Introduction and Motivation

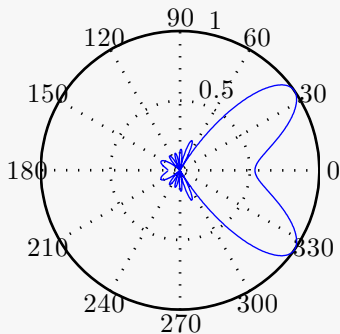
Narrowband Beamforming

UWB Beamforming

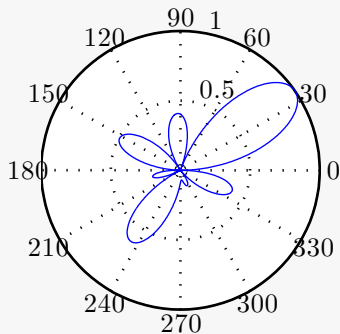
Simulation Process

Future Work

## Linear Array



## Circular Array



$$\phi_o = 35$$

# Comparison bet. Linear and Circular Array Radiation Patterns



Circular antenna array beamforming for UWB

Mohammed Shalaby

Contents

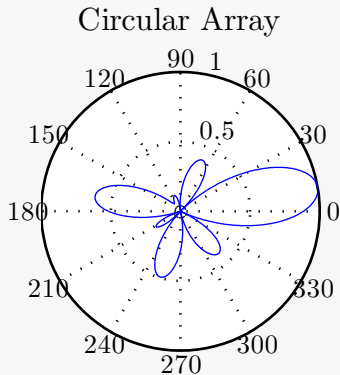
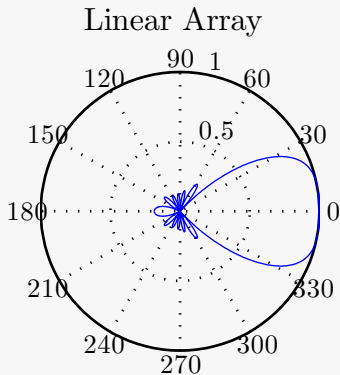
Introduction and Motivation

Narrowband Beamforming

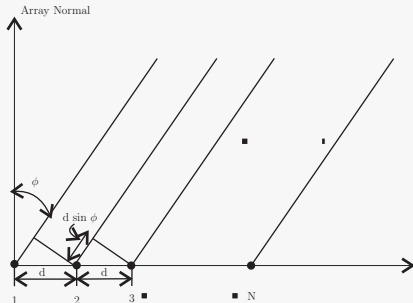
UWB Beamforming

Simulation Process

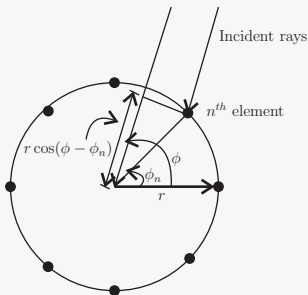
Future Work



$$\phi_o = 10$$

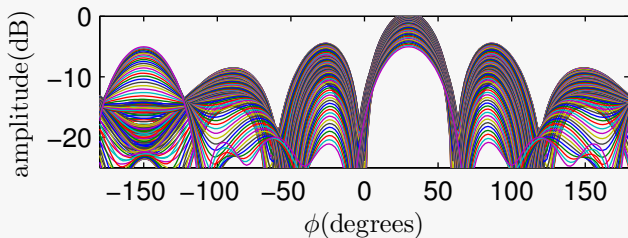


$$AF = 1 + \exp \{jkd \sin \phi\} + \dots = \sum_{n=1}^N \exp \{j(n-1)kd \sin \phi\}$$

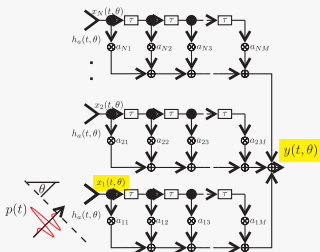


$$AF_c = \sum_{n=1}^N \exp \{jkr \cos(\phi - \phi_n)\}$$

- $\phi_n = \frac{2\pi(n-1)}{N}$
- Assumption: the elevation angle  $\theta = 90$



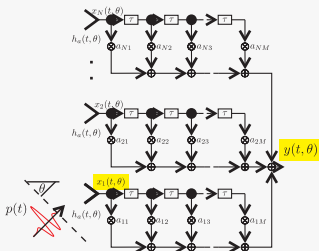
- UWB signal has a very wide bandwidth
- *Each* frequency in that band generates its own radiation pattern as seen in the diagram which is undesired
- Additional Degree of freedom is needed to ensure frequency independency
- Digital solution is not yet possible as current samplers do not offer the need sampling rates



## Advantages of FIR based Arrays

- They are easy to realize as a typical FIR branch consists of *delay elements* which can be implemented using microstrip lines and *multipliers* which can be implemented using FET Technology, thus eliminating the need for the complex phase-shifting circuits used in the narrowband case.

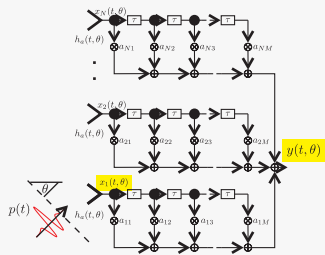




## Advantages of FIR based Arrays

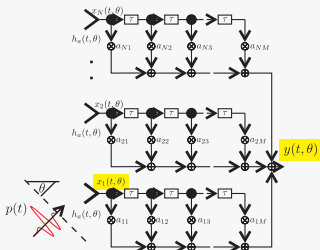
- The array physical size is compact as the inter-element spacing  $d$  is determined by

$$d \leq \frac{c}{2f_h}$$



## Advantages of FIR based Arrays

- Since it has wideband properties, it eliminates the need for different antenna spacing for applications involving various carrier frequencies.



## Advantages of FIR based Arrays

- They can compensate for the frequency responses of the transmitting antenna, receiving antenna and channel (Equalization), so the pulse shape is faithfully reproduced.

## Procedure to determine the coefficients of the FIR filter

- 1 we first equate the desired radiation pattern  $H_d(f, \phi)$  to the array radiation pattern  $H_{arr}(f, \phi)$

$$H_{arr}(f, \phi) = \sum_{n=1}^N \sum_{m=1}^M a_{nm} \exp \{ -j2\pi f [(n-1)\tau_o + (m-1)\tau] \}$$

- 2 careful examination of equation 4.2.6 reveals that it looks like a DFT. Thus, by choosing preliminary  $N$  and  $M$  and applying the IDFT, we get the sought-after coefficients  $a_{nm}$
- 3 we autocorrelate the desired radiation pattern  $H_d$  and the radiation pattern constructed using the coefficients from step 2 and see whether they are similar enough (a criteria should be defined for that), if not step 2 should be repeated with different values of  $M$  and  $N$  until a satisfactory result

Circular antenna array beamforming for UWB

Mohammed Shalaby

Contents

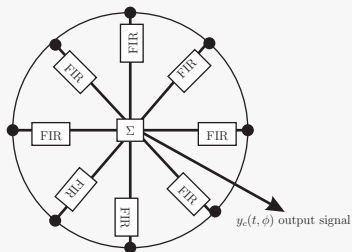
Introduction and Motivation

Narrowband Beamforming

UWB Beamforming

Simulation Process

Future Work



## Time-Domain output signal

$$y_c(t, \phi) = p(t) * \sum_{n=1}^N \sum_{m=1}^M a_{nm} \delta(t - (m-1)\tau) * (t - ((r/c) \cos(\phi - \phi_n)))$$

where  $\phi_n = \frac{2\pi(n-1)}{N}$

## Frequency-Domain output signal

$$Y_c(f, \phi) = \sum_{n=1}^N \sum_{m=1}^M a_{nm} \exp \{ -j2\pi f [(m-1)\tau + (r/c) \cos(\phi - \phi_n)] \}$$

where  $\phi_n = \frac{2\pi(n-1)}{N}$

- Power of the exponential function not a linear function of  $n$   
 $\Rightarrow$  IDFT can not be applied to calculate the coefficients
- attempts to linearize the cosine function  
 $\Rightarrow$  proves to be very complicated  
 $\Rightarrow$  that's why a numerical solution is preferred

The influence of the following parameters will be investigated:

- The number of the antenna elements  $N$
- The order of the FIR filters  $M$

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- The bandwidth of input pulse



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- The bandwidth of input pulse
- The radius of the circular array  $r$

Finally a Time-Domain example is given to give an impression of the whole Procedure involving typical Parameters.

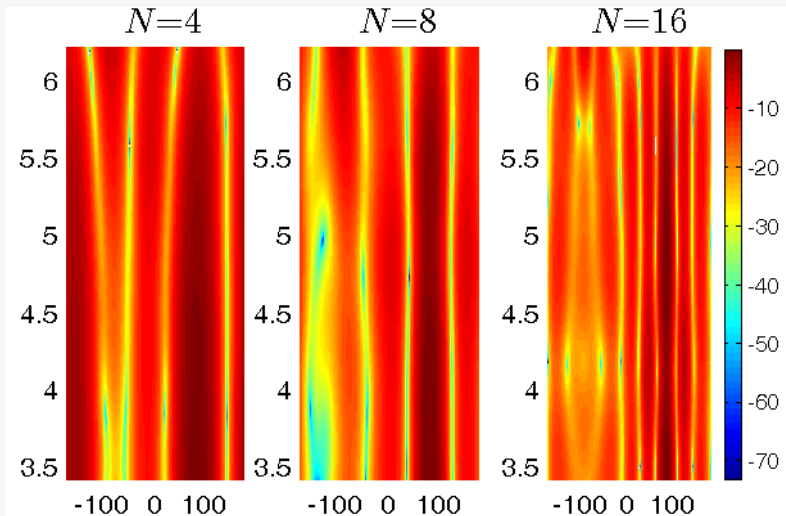
## simulation conditions

3 circular arrays are compared with same:

- radius  $r$
- filter order  $M = 8$
- target angle  $\phi_o = 80^\circ$
- signal bandwidth  $f_h = 2f_l$  where  $f_l = 3.1$  GHz

but with different number of antenna elements  $N =$

- 4
- 8
- 16



## Conclusions

As the number of antenna elements  $N$  increases:

- The mainlobe narrows
- The number of sidelobes increases
- Their peak level decreases
- At some value of  $N$  saturation is reached

Note:  $N$  can not be arbitrarily increased for a fixed radius because of the limitations imposed by the antenna size and the mutual coupling

## simulation conditions

3 circular arrays are compared with same:

- radius  $r$
- number of antenna elements  $N = 16$
- target angle  $\phi_o = 30^\circ$
- signal bandwidth  $f_h = 3f_l$  where  $f_l = 3.1$  GHz

but with different filter order  $M =$

- 8
- 12
- 16

# Variation of the order of the FIR filters $M$

Circular  
antenna  
array  
beamforming  
for UWB

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Contents

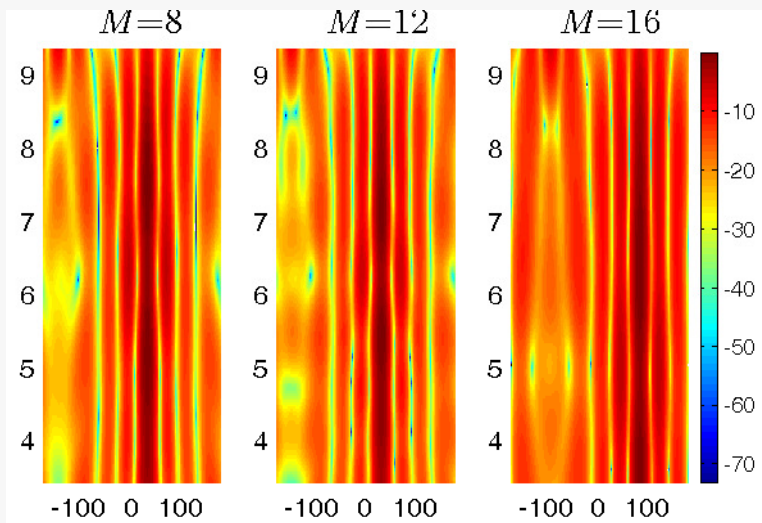
Introduction  
and  
Motivation

Narrowband  
Beamforming

UWB  
Beamforming

Simulation  
Process

Future Work







# Variation of the order of the FIR filters $M$

Circular  
antenna  
array  
beamforming  
for UWB

Mohammed  
Shalaby

Contents

Introduction  
and  
Motivation

Narrowband  
Beamforming

UWB  
Beamforming

Simulation  
Process

Future Work

## Conclusions

As the Filter Order  $M$  increases:

- The deviation from the desired radiation pattern decreases
- Frequency independency increases
- At some value of  $M$  saturation is reached

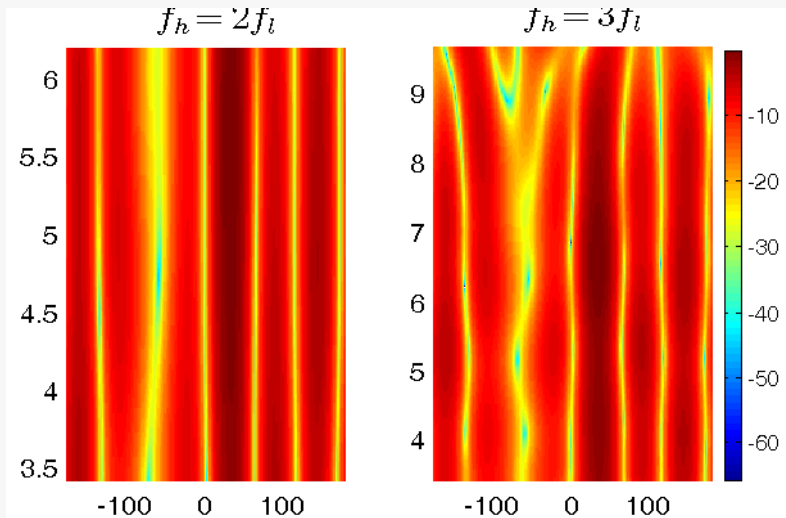
## simulation conditions

2 circular arrays are compared with same:

- radius  $r$
- number of antenna elements  $N = 8$
- target angle  $\phi_o = 30^\circ$
- filter order  $M = 8$

but with different relative bandwidth=

- $f_h = 2f_l$
- $f_h = 3f_l$





# Variation of the bandwidth of input pulse

Circular  
antenna  
array  
beamforming  
for UWB

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Shalaby

Contents

Introduction  
and  
Motivation

Narrowband  
Beamforming

UWB  
Beamforming

Simulation  
Process

Future Work

## Conclusions

As the bandwidth of the input pulse increases:

- Frequency independency decreases especially at the edges of the band
- Higher Filter order is needed

## simulation conditions

3 circular arrays are compared with same:

- number of antenna elements  $N = 8$
- target angle  $\phi_o = 30^\circ$
- filter order  $M = 8$
- relative bandwidth  $f_h = 2f_l$

but with different radius  $r =$

- $r_{max}$  where  $r_{max}$  is  $\frac{c}{2f_h \sin(\frac{2\pi}{N})}$
- $0.75 r_{max}$
- $0.5 r_{max}$

# Variation of the radius of the circular array $r$

Circular  
antenna  
array  
beamforming  
for UWB

Mohammed  
Shalaby

Contents

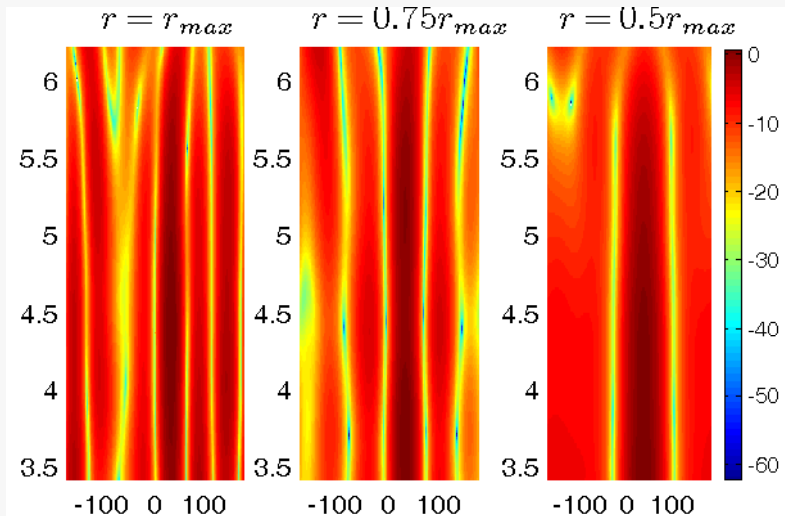
Introduction  
and  
Motivation

Narrowband  
Beamforming

UWB  
Beamforming

Simulation  
Process

Future Work





# Variation of the radius of the circular array $r$

Circular  
antenna  
array

beamforming  
for UWB

Mohammed  
Shalaby

Contents

Introduction  
and  
Motivation

Narrowband  
Beamforming

UWB  
Beamforming

Simulation  
Process

Future Work

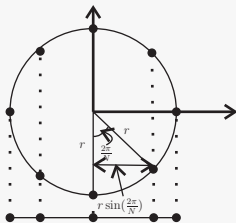
## Conclusions

As the radius of the antenna elements  $r$  decreases:

- The number of sidelobes decrease
- The the mainbeam widens

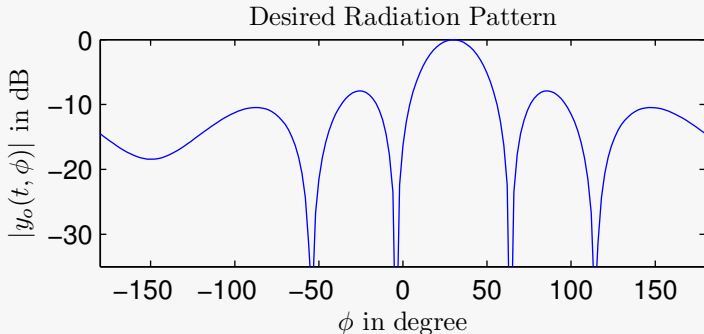
- Circular arrays have the inherent characteristics of the presence of undesired higher sidelobe levels compared to linear arrays
- That can be minimized by exerting a limit on the maximum interelement spacing and hence a maximum radius as well
- According to [Balanis 2004] the maximum interelement spacing is the arc  $\frac{2\pi r}{N}$ .  
⇒ not convincing
- I suggested that  $r_{max}$  is  $\frac{c}{2f_h \sin(\frac{2\pi}{N})}$  according to the following diagram.





- Not totally *physically* correct due to the double weighting and interference of opposite elements but *mathematically* correct as long as it is less and not less than or equal
- with a radii in the order 1-2 cm the maneuvering space is very limited due to the antenna physical size
- Smart engineering sense is needed for estimation

GOAL  $\Rightarrow$  to realize a Radiation Pattern for a short pulse application using a FIR Circular array. This Broadband Radiation Pattern should resemble (as far as possible) a desired Radiation Pattern of a Narrowband Circular Array with number of antenna elements  $N=16$ .





# Typical Time-Domain Example

Circular  
antenna  
array  
beamforming  
for UWB

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Contents

Introduction  
and  
Motivation

Narrowband  
Beamforming

UWB  
Beamforming

Simulation  
Process

Future Work

## Procedure

- 1 The number of antenna Elements  $N$  is given.
- 2  $f_l$  and  $f_h$  are determined by the -10 dB marks of the Fourier transformed pulse



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Circular  
antenna  
array  
beamforming  
for UWB

Mohammed  
Shalaby

Contents

Introduction  
and  
Motivation

Narrowband  
Beamforming

UWB  
Beamforming

Simulation  
Process

Future Work

## Procedure

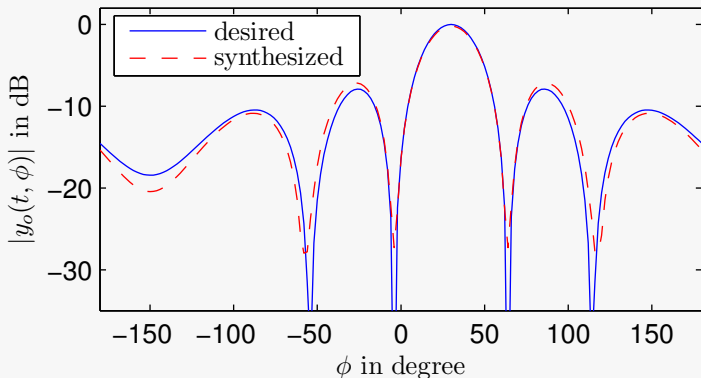
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- 5 Step 4 is repeated with different values of  $M$  until a satisfactory result is reached

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- $N = 16; \phi_o = 30^\circ$
- $f_h = 3 f_l$  where  $f_l = 3.1$  GHz
- $M = 14; r = 0.016$  m



Circular  
antenna  
array  
beamforming  
for UWB

Mohammed  
Shalaby

Contents

Introduction  
and  
Motivation

Narrowband  
Beamforming

UWB  
Beamforming

Simulation  
Process

Future Work

- Investigate the influence of the real antenna in terms of physical size, frequency characteristic and mutual coupling
- Try to find an analytical solution for circular arrays





Circular  
antenna  
array  
beamforming  
for UWB

Mohammed  
Shalaby

Contents

Introduction  
and  
Motivation

Narrowband  
Beamforming

UWB  
Beamforming

Simulation  
Process

Future Work

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Circular  
antenna  
array  
beamforming  
for UWB

Mohammed  
Shalaby

Contents

Introduction  
and  
Motivation

Narrowband  
Beamforming

UWB  
Beamforming

Simulation  
Process

Future Work

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Circular  
antenna  
array  
beamforming  
for UWB

Mohammed  
Shalaby

Contents

Introduction  
and  
Motivation

Narrowband  
Beamforming

UWB  
Beamforming

Simulation  
Process

Future Work

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- Examine other geometries, for instance: elliptical arrays
- Choose a phase reference other than the array center
- Investigate the effect of the tolerances of electronic components



Circular  
antenna  
array  
beamforming  
for UWB

Mohammed  
Shalaby

Contents

Introduction  
and  
Motivation

Narrowband  
Beamforming

UWB  
Beamforming

Simulation  
Process

Future Work

- Investigate the influence of the real antenna in terms of physical size, frequency characteristic and mutual coupling
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# Acknowledgments

Circular  
antenna  
array  
beamforming  
for UWB

Mohammed  
Shalaby

Contents

Introduction  
and  
Motivation

Narrowband  
Beamforming

UWB  
Beamforming

Simulation  
Process

Future Work

I would like to thank Prof.Solbach for letting me do my thesis in his institute under his supervision.

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Last but not least I would like to thank the audience for their attention

Circular  
antenna  
array  
beamforming  
for UWB

Mohammed  
Shalaby

Contents

Introduction  
and  
Motivation

Narrowband  
Beamforming

UWB  
Beamforming

Simulation  
Process

Future Work

